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Multi-beam modulated metasurface antenna for 5G backhaul applications at K-band

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1. Introduction

Microwaves and millimeter waves frequencies are among the frequency bands allocated for small-cell backhaul in 5G networks [1]. The use of metasurfaces (MTSs) for 5G systems has been studied and proved to be extremely useful in the aforementioned frequency ranges. Indeed, some antenna prototypes based on MTSs have already been developed with the aim of satisfying the needs of the new generation of mobile networks [2, 3]. Modulated MTS antennas, which were initially developed for satellite communications, are a special category of MTS antennas [4].
low profile, low cost and reduced power consumption of this kind of structures, along with the adaptability of the design process to different frequencies, make them a very attractive solution.

A MTS is generally formed by sub-wavelength elements arranged on a periodic lattice and either printed on a grounded dielectric slab or grown on a metallic base-plate. By changing the geometry of these constitutive elements in the lattice unit-cell, one can exert a high degree of control on the aperture fields [5–7]. The MTS layer can be modeled as a continuous impedance boundary condition (IBC) due to the small size of the elements compared to the wavelength. In modulated MTS antennas, a surface wave (SW) is excited on the aperture and gradually transformed into a leaky-wave owing to its interaction with the periodically modulated IBC, which results in a radiated beam [8]. By tuning the properties of the modulation one can control the attributes of the beam, such as the pointing angle, shape, and polarization.

This paper presents a modulated MTS antenna operating at K-band with multibeam performance. The system is based on a pillbox quasi-optical beamformer [9], which essentially transforms the cylindrical wave propagating on the pillbox’s lower layer into a plane wave in the upper layer. By adding a modulated MTS on the top layer (Figure 1), one obtains a compact antenna. A pillbox-fed modulated MTS antenna at X-band was described in [10]. As mentioned before, the entire design process can be adapted for other frequency bands by properly modifying the material, the beamformer, and the MTS elements dimensions. Thus, in this work, we use a strategy similar to that described in [10] to design an antenna operating at \( f_o = 20.7 \) GHz.
2. Design of a multi-beam modulated metasurface antenna

In the following, we will refer to the Cartesian reference system \((x, y, z)\) shown in Figure 1. The IBC used to model our MTS consists in a sheet transition [11, 12], penetrable [13] or transparent impedance [14, 15] \(Z_s = jX_s\) which lies on top of a grounded dielectric slab. This structure supports the propagation of a TM surface wave. In order to get the desired radiation effect, the sheet transition impedance is modulated along \(x\)-direction as

\[
X_s(x) = X_{av}(1 + M(x) \cos(2\pi x / p)),
\]

where \(X_{av}\) is the average reactance, \(M(x)\) is the modulation index \((0 \leq M(x) \leq 1)\) and \(p\) is the period. The chosen material is Rogers RO3006 \((\varepsilon_r = 6.15, \tan\delta = 0.002)\) with thickness \(h = 0.64\) mm. In order to implement (1), we use square metallic patches whose size changes according to the spatial variation of \(X_s(x)\). To that end, we first build a database that relates the patch dimensions to the sheet transition IBC values. Taking a unit-cell (a single MTS element) of side \(a\) on a substrate of thickness \(h\), and assuming it inside a regular lattice to preserve the local periodicity principle, one can vary progressively the metallic patch size \(s\) and extract the equivalent sheet impedance \(Z_s\). Figure 2 shows the curve that relates both parameters as well as an inset with the geometry of the unit-cell. The MTS element has a constant size \(a = \lambda_0 / 7\), which makes it small compared to the SW wavelength, as indicated in Section 1. Once we have characterized the unit-cell, the next design step consists in retrieving the square patch dimensions that better match the ideal values in (1) to obtain our modulated MTS. The latter is placed then on the beamformer top layer to get the final structure depicted in Figure 3.

In addition, it is important to note that the use of a pillbox allows one to place several sources (here, H-plane horns) in the bottom layer. These horns are arranged at the focal plane of the pillbox’s reflector (Figure 3) and each one provides a beam pointing at a different direction. Indeed, when the source position is shifted in the focal plane (along \(y\)-direction), the direction of propagation of the resulting plane-wave changes. As a result, the placement of \(N\) ports originates up to \(N\) beams at different pointing angles. This feature will be illustrated in the next section. Obviously, the number of sources is limited by the pillbox dimension, the horn size, and the HPBW of the radiated beams. The antenna dimensions are sketched in Figures 1 and 3, from where we emphasize a very low profile, with a total thickness of 1.28 mm.

The main advantage of operating at a higher frequency with respect to the X-band model in [10] is the reduction of the antenna dimensions. First, for the require bandwidth, it is possible...
to employ a thinner substrate that keeps providing the needed impedance range (Figure 2), which
enforces the low-profile faculty of the system. The total radiating aperture size is also decreased,
going up to almost a 50% smaller area than that in the X-band design. Another important aspect
is the diminution of the feeding horn width, since the cut-off frequency is now larger. This allows
one to set more sources along the pillbox focal plane and, hence, the number of beams on the
scanning region is increased. The latter point is commented and exploited in Section 3.

In order to overcome the losses growth due to the frequency rise, the length of the lower layer
is shortened (Figure 1). This is traduced into a minimization of the pillbox focal distance, while
ensuring the required performance for the side lobe level (SLL ≤ −15 dB) and the beam-width
at −3 dB (HPBW = 5°). Such a modification is realized by adjusting the horn dimensions and the
pillbox reflector diameter.

The proposed design is a good alternative to phased array antennas [16, 17]. In fact, the ab-
sence of phase-shifters makes our MTS antenna simpler, cheaper and less power-consuming.
Furthermore, the structure can be fabricated using PCB technology, which facilitates the manu-
facturing process and reduces the cost.

3. Simulation results

For the design at hand, we implement (1) to obtain a beam at θ₀ = 15° for normal incidence (port
1, φ₀ = 0°). The employed modulation parameters are p = 11.3 mm, Xav = −0.24η₀ (where η₀
is the free-space impedance), and M varying with x to optimize the attenuation of the aperture
fields and, therefore, enhance the aperture efficiency of the antenna [18]. Switching between the
N = 7 ports implies the modification of both θ₀ and φ₀. The simulated S-parameters of the horns
are shown in Figure 4, revealing a bandwidth of 20% and a very good isolation between ports.

Figure 5 presents the radiated beams for each source at f₀. The obtained angular coverage
is displayed in Figure 5a, where the direction of the beam is given in (θ, φ) coordinates. Next,
we represent in Figure 5b the radiation pattern in elevation at the E-plane for every port. The
patterns are plotted by cutting every 3D beam at the angle φ = φ₀, where φ₀ is the azimuth angle
of maximum gain for each source. The maximum realized gain at f₀ is G = 27.1 dB for port 1 and
the beam-switching losses are up to 2.5 dB (realized gain difference between port 1 and ports 4, 7).
We note that the generated beams own the property of frequency scanning in θ. Thus, it would
Figure 5. (a) Radiation performance in ($\theta, \phi$) plane, and (b) realized gain at the E-plane cut for each horn.

be possible to operate at other frequencies around $f_o$ within the bandwidth shown in Figure 4, modifying then the individual beam directions and the angular coverage.

The described model is under fabrication and a measuring experiment is planned. Besides, the scanning area can be extended to the region $\theta < 0^\circ$ (Figure 5a) by arranging an additional reflector and horns opposed in the x-axis to the existing ones [19].

4. Conclusion

We presented the design and numerical results of a compact modulated MTS antenna at 20.7 GHz. The radiating aperture consists of metallic patches whose size is modified to produce an equivalent modulated impedance. The MTS antenna is fed by a plane SW, which is obtained by means of a quasi-optical beamformer in a pillbox architecture. Moreover, one can change the propagation direction of this SW by exciting different ports in the pillbox focal plane. The proposed antenna topology is able to generate high-gain beams at different pointing angles, while providing a good scanning range in $\theta$ and a wide angular coverage in $\phi$. The extremely thin profile of the structure ($h_{total} = 1.28$ mm), the high-gain behavior, and the multi-beam capability make this antenna a suitable candidate for backhaul applications. Last but not least, this flat
aperture antenna can be easily integrated with a low visual impact on smart urban furniture, buildings, homes, and offices.

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